Compact wide stopband microstrip lowpass filter using polygon patches and meandered lines

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Abstract

In this paper, a low pass filter based on T-Shaped resonator is presented. The T-Shaped resonator consists of meandered lines and rectangular patches. Also, the LC model and transfer function of the proposed resonator is presented. For suppression of spurious harmonics, a bandstop structure consists of hexagonal patches and open stubs has been utilized. Finally, the wide stopband microstrip lowpass filter with cutoff frequency 2.72 GHz has been simulated, fabricated and measured. The LPF has good characteristics such as wide stopband and insertion loss lower than 0.18 dB in the passband region. The rejection level is less than $-20$ dB from 2.98 up to 21.3 GHz. The filter size is $10.5 \text{ mm} \times 12.7 \text{ mm}$, or $0.131 \lambda_g \times 0.158 \lambda_g$, where $\lambda_g$ is the guided wavelength. The measured and simulated results of the filter is in good agreement with each other, which show the merits of low insertion loss and wide stopband.

Keywords:
Lowpass filter
Meandered line
Patches
T-shaped resonator

1. INTRODUCTION

The lowpass filters (LPFs) are used in the communication systems for elimination of undesired frequencies. There are several requirements for a LPF such as small size, low loss in passband region, and wide stopband. Planar filters have attracted considerable attention due to low cost, simple structures and capability of integration with other microwave circuits [1]. To suppress the spurious frequencies, the stepped impedance filters were introduced in [2-3]. To have high order harmonic suppression, stepped impedance hairpin resonator was proposed in [2]. In [3], a compact low pass filter with widestop band by using transformed stepped impedance resonator, was proposed. However, the reported work in [3] has poor selectivity from passband to stopband region. Other methods such as defected ground structure (DGS) and slotted structure to design of filters have been proposed, but the main problem is complexity of fabrication process [4-7]. In [4], the bandwidth of filter has been increased by a DGS structure. The filter based on DGS in [5] has wide stopband. Yet, it provides high insertion loss and gradual cutoff frequency. Also, multi-stopband filter based on tree fractal slotted structure in [6] and LPF using DGS in [7] have been proposed. The microstrip lowpass filters with compact size and ultrawide stopband using triangular and polygonal patch resonator are presented in [8] which have poor selectivity. In [9], multimode resonators to design of wide stopband LPF with high selectivity have been used. However, the multimode LPF has the stopband region with low attenuation level. In [10], a novel design of a LPF based on metamaterial was introduced. The proposed filter is investigated based on square split ring resonators (SRRs) with good attenuation level in the stopband but suffers from low stop bandwidth and large size. In [11], the presented filter used meandered
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To deal with problems such as low selectivity, narrow stopband, high insertion loss, and large size, a new microstrip lowpass filter with good performance has been presented in this work. This paper, addresses all those problems by obtaining wide stopband by bandstop structure instead of cascaded resonators since cascaded resonators result in size increasing. From the proposed design, it is found that there is only optimum number of elements to maximize filter stopband and minimize passband losses.

The rejection level better than −20 dB is obtained in the range of 2.98 up to 21.3 GHz. The filter size is 10.5 mm×12.7 mm, or 0.131 λg× 0.158 λg, where λg is guided wavelength. Measured results of the developed lowpass filter are in good agreement with the simulation ones, thereby proving the validity of the proposed filter. The paper is organized as the following. In the first section, we provide an overview of the proposed resonator with lumped and distributed elements. In the second section, we argue the bandstop structure based on lumped and distributed elements. The LPF design and the obtained results are presented in third and fourth sections, respectively. Finally, the conclusion is presented in the fifth section.

2. DESIGN OF RESONATOR

A new T-shaped resonator using meandered line is presented. Meandered lines are employed and loaded with rectangular patches to achieve the high selectivity and low insertion loss. In Figure 1(a) and (b), the layout and equivalent circuit of basic resonator consists of meandered line and rectangular patch is shown.

![Figure 1. (a) Layout, (b) Equivalent circuit, and (c) Simulated S-parameters](image)

In Figure 1(b), \( L_1 \) and \( C_1 \) are inductance and capacitance of high impedance transmission lines. \( L_2 \) is inductance of meandered line, which is assumed lossless, and \( C_2 \) refers to the capacitance of the rectangular patch. The values of inductors and capacitors can be obtained from (1)-(3) as

\[
L_i = \frac{1}{\omega} Z_{si} \sin \left( \frac{2\pi}{\lambda_g} l_i \right) \tag{1}
\]

and

\[
C_i = \frac{1}{\omega} \frac{1}{Z_{si}} \tan \left( \frac{\pi}{\lambda_g} l_i \right) \tag{2}
\]

and the capacitance of the open stub is

\[
C_{oi} = \frac{\sqrt{\varepsilon_{eff}} l_i}{c Z_{si}} \tag{3}
\]

where \( Z_{si} \) is the characteristic impedance of the line, \( l_i \) is its length, \( c \) is the velocity of light in free space and \( \lambda_g \) is the guided wavelength at the cut-off frequency. The values of these parameters after optimization obtained as \( L_1=3.1 \) nH, \( L_2=3.05 \) nH, \( C_1=0.07 \) pF, and \( C_2=0.8 \) pF. The dimensions are \( l_1=5.25 \) mm, \( l_2=1 \) mm, \( l_3=0.6 \) mm, \( w_1=3.9 \) mm, \( w_2=4.1 \) mm, and \( w_3=0.4 \) mm. Figure 1(c) shows the LC and EM simulation results of the basic resonator. As it is illustrated, the agreement between LC and EM simulation results has been met perfectly. The \( S_{21} \) parameter of the basic resonator shows that the resonator has low rejection level in the stopband. Also, the transmission zero (TZ) of the basic resonator is 3.15 GHz, which is obtained as...
\[ T_1(s) = \frac{Z_0(C_2L_2s^2+1)}{C_1C_2L_1L_2s^4+(L_1(C_1+C_2)+C_2L_2(2-Z_0))s^2+(2-Z_0)} \]  

(4)

Hence, the position of transmission zero, \( f_z \), can be determined by setting the \( T_1(s) = 0 \), which results in \( f_z = 3.3 \) GHz. Also, the variation of cut-off frequency of the basic resonator versus \( w_2 \) and \( l_2 \) parameters is shown in Figure 2(a) and 2(b), respectively. As it can be seen, the cutoff frequency has been decreased by increasing \( w_2 \) and \( l_2 \). By varying the dimensions of the patch structure, the cutoff frequency of the proposed resonator can be tuned.

Figure 2. Cut-off frequency versus (a) \( w_2 \) and (b) \( l_2 \)

Figure 3(a) and 3(b) show the proposed resonator and its equivalent LC circuit. The S-parameters of the proposed resonator and LC model is shown in Figure 3(c). It can be seen from Figure 3(d), the transmission zero is shifted from 4.6 GHz up to 3.3 GHz by increasing \( w_2 \). The transfer function (TF) of the proposed resonator is obtained as

\[ T_2(s) = \frac{Z_0(C_2L_2s^2+1)}{C_1C_2L_1L_2s^4+(L_1(C_1+C_2)+C_2L_2(2-Z_0))s^2+(2-Z_0)} \]  

(5)

From (5), \( f_z = 3.3 \) GHz is obtained.

Figure 3. (a) Layout, (b) LC equivalent circuit, (c) Simulated S-parameters, and (d) simulated S\(_{21}\) parameter versus \( w_2 \)
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3. DESIGN OF BANDSTOP STRUCTURE

The bandstop structure (BSF) are designed based on two open stubs and high impedance line loaded by four hexagonal patches (resonator-II). The main section is a high impedance line having an impedance of 134 Ω connected in series with a hexagonal patch. The resonator-II has been designed and simulated with the Advanced Design System (ADS). When the layout of the resonator has been generated, an electromagnetic momentum (EM) simulation has been carried out to analyze its performance. Its layout and LC equivalent circuit is shown in Figure 4. The dimensions are \( l_4 = 3.13 \) mm, and \( l_5 = 1.7 \) mm. This unit has one transmission zero at 8 GHz with attenuation level -43 dB.

The configuration, LC equivalent circuit and simulated characteristics of two units are shown in Figure 5(a), 5(b) and 5(c), respectively. For the analysis of equivalent circuit, the hexagonal high frequency, the inductance of main high impedance line blocks the transmission of unwanted harmonics and improved stop bandwidth.

![Figure 4. (a) Layout, and (b) Equivalent circuit of resonator-II](image)

From (6), \( f_{21}=7.9 \) GHz and \( f_{22}=8.5 \) GHz is obtained. By connecting two units symmetrically connected at the centre of main high impedance transmission line, the structure in Figure 6 (a) is obtained. Figure 6(b) exhibits two transmission zeros, which are located at about 7.67 GHz and 9 GHz with attenuation level near -62 dB and -60 dB. These transmission zeros are caused by the resonance of the high impedance single stepped stub loaded by triangular patches and its resonant frequency depends on the structural parameters.

In practical applications, a filter with wide stopband and high suppression level is necessary. The bandwidth of the proposed filter can be enhanced by connecting open stubs on both sides of the resonators. The layout and frequency response of two open stubs are shown in Figure 7. The open stub produces a transmission zero to eliminate the harmonic at 14 GHz. The filter using open circuit stub at both ends of the high impedance main transmission line exhibits better stopband characteristics. The length and width of the open stub are \( l_5=10.2 \) mm and \( w_5=1.17 \) mm, respectively. Each open stub can be considered as a shunt capacitor to the ground. At high frequencies, the capacitive reactance decreases, and open stub acts as a short circuit to the ground. This shorts out transmission and causes attenuation in the stopband which suppresses the higher frequency harmonics and extends the stopband.

The bandstop unit in Figure 8(a) has been added to the resonator. The \( S_{21} \) parameters of bandstop structure are depicted in Figure 8(b). At high frequency, the inductance of main high impedance line blocks transmission by having infinite series reactance, whereas the capacitance of open stub shorts out transmission by having infinite shunt susceptance. The rejection level from 4 up to 14 GHz is better than -15 dB. So, the undesired passband at 14 GHz has been diminished. This clearly indicates the ability of the bandstop structure to elimination of unwanted harmonics and improved stop bandwidth.
4. FILTER DESIGN AND LAYOUT

The schematic showing the generation process of the proposed filter on substrate with the permittivity of 2.2, loss tangent of 0.0009 and thickness of 0.508 mm is given in Figure 9(a). The LPF occupies 10.5 mm×12.7 mm. Fig 9(b) shows the photograph of the fabricated filter. Addition of bandstop structure to the proposed resonator results in good rejection level in the stopband region. The proposed
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5. RESULTS AND DISCUSSION

Figure 10(b) shows the measured and simulated S-parameters of the proposed LPF. One transmission zero is located at 2.97 GHz to have high selectivity. In addition, extra transmission zeroes in the stopband region can be observed. In general, these transmission zeros help us in out-of-band rejection enhancement. The measured insertion loss is less than 0.18 dB, while the return loss is greater than 12.5 dB from DC up to 3.39 GHz. The simulated group delay is shown in Figure 10(c). It can be seen that the group delay is less than 0.32 ns in the passband. Furthermore, over 20 dB attenuation level in the stopband region is achieved from 2.98 up to 21.3 GHz, so that the unwanted signal is eliminated. For comparisons, Table 1 illustrates the measured results for some previous works and proposed filter, where roll off rate $\zeta$ is defined as

$$\zeta = \frac{\alpha_{\text{max}} - \alpha_{\text{min}}}{f_c - f_s}$$ (7)

where $\alpha_{\text{max}}$ and $\alpha_{\text{min}}$ represent the $-20$ dB and $-3$ dB attenuation level, respectively, $f_c$ is the $-3$ dB cutoff frequency, and $f_s$ is the $-20$ dB stopband frequency. In this case, the bandwidth divided by center frequency of stopband is the relative stopband width (RSB) as

$$\text{RSB} = \frac{\text{stopband bandwidth}}{\text{stopband centre frequency}}$$ (8)

The rejection level divided by 10 is suppression factor (SF), which is defined as

$$SF = \frac{\text{rejection level}}{10}$$ (9)

As an example, the SF of the proposed LPF with rejection levels of 20 dB is 2. The normalized circuit size (NCS) is defined as
Comparing with the other filters [2-3, 5], [7-11], clearly a transmission zero close to the passband is realized with T-shaped resonator and the filter has sharp roll-off rate in comparison to [2-3, 5], [7-11]. Moreover, the stop bandwidth of the proposed filter can be further extended by using Split Ring Resonators as [7]. Also, the proposed filter has lower insertion loss in comparison to other works. However, the filter is symmetrical and miniaturized in dimension which is less costly to implement in communication applications. The measured and simulated results of the filter have good agreement at lower frequency. The difference at high frequencies is due to the imperfect soldering of the ports and inaccurate implementation of the proposed filter.

**Table 1. Comparison of the proposed LPF with other works.**

<table>
<thead>
<tr>
<th>Ref</th>
<th>$\zeta$</th>
<th>RSB</th>
<th>SF</th>
<th>Insertion Loss</th>
<th>NCS</th>
</tr>
</thead>
<tbody>
<tr>
<td>[2]</td>
<td>52.8</td>
<td>1.53</td>
<td>2</td>
<td>0.5</td>
<td>0.113+0.081</td>
</tr>
<tr>
<td>[3]</td>
<td>14.1</td>
<td>1.54</td>
<td>1.4</td>
<td>0.4</td>
<td>0.103+0.071</td>
</tr>
<tr>
<td>[5]</td>
<td>43.9</td>
<td>1.355</td>
<td>1.5</td>
<td>1</td>
<td>0.15+0.101</td>
</tr>
<tr>
<td>[7]</td>
<td>20</td>
<td>1.65</td>
<td>1.7</td>
<td>0.3</td>
<td>0.12+0.071</td>
</tr>
<tr>
<td>[8]</td>
<td>16.66</td>
<td>1.55</td>
<td>1.5</td>
<td>0.36</td>
<td>0.081+0.089</td>
</tr>
<tr>
<td>[9]</td>
<td>15</td>
<td>1.58</td>
<td>1.5</td>
<td>0.5</td>
<td>0.11+0.09</td>
</tr>
<tr>
<td>[10]</td>
<td>17</td>
<td>1</td>
<td>2</td>
<td>0.2</td>
<td>0.11+0.11</td>
</tr>
<tr>
<td>[11]</td>
<td>56.7</td>
<td>1.267</td>
<td>2</td>
<td>0.3</td>
<td>0.116+0.115</td>
</tr>
<tr>
<td>This work</td>
<td>65.4</td>
<td>1.54</td>
<td>2</td>
<td>0.18</td>
<td>0.158+0.131</td>
</tr>
</tbody>
</table>

6. CONCLUSION

An LPF with cutoff frequency 2.72 GHz by modified T-shaped resonator has been designed, fabricated, and measured. To improve the stopband bandwidth, the bandstop structure consists of using open stubs and hexagonal patches has been added at the two sides of the proposed resonator. An approximate LC equivalent circuit of each structure has been derived and its response has been compared with simulated result. A high attenuation over the stopband up to 21.3 GHz has been obtained so that the unwanted out-of-band signal is eliminated. The obtained results show that the proposed filter has good performance such as low insertion loss, wide stopband and high selectivity in comparison to other filters. Due to compact size, low insertion loss and wide stopband, the proposed LPF is expected to be applied in modern wireless communication systems.

REFERENCES


\[
NCS = \frac{\text{physical size} \times \text{width}}{\lambda_0} \tag{10}
\]